

A Ku-band SIW Six-port

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ABSTRACT

This paper shows a compact fully integrated six-port Substrate Integrated Waveguide (SIW) operating at Ku-Band frequency range. The SIW six-port is formed by combining two SIW power dividers and two SIW couplers, having the benefit of no additional termination is required as this topology has no excessive port. To achieve the optimized design of the six-port, both of the key components; power divider and coupler are primarily designed, fabricated, and measured individually. Y-junction topology is employed on the power divider structure to achieve a compact size. In turn, the coupling coefficient of the two output ports of the SIW coupler are improved by shifting the position of a row of several vias located at the side wall center closer to the side wall. The simulated six port performance provides an advantage of wide bandwidth within Ku-Band across 13 to 17 GHz with a return loss better than 12 dB and transmission coefficient of 7 ± 1.5 dB. The simulated and measured results show good agreement thus validating the prototype. The SIW six-port can find its application in designing a six-port.

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1. INTRODUCTION

The common radar based sensor faces design challenges at high frequency. The six-port interferometer proposed for short range radar based system has shown several advantages compared to the traditional device [1-2]. The six-port interferometer has the advantage of a lower complexity design process at any operating frequency with a wider bandwidth because the structure is constructed by passive components [3].

Generally, the six-port interferometer is formed by the interconnection of power dividers, couplers, and phase shifters [4-5]. Compared to the traditional coaxial cavities or microstrip technique, SIW is known to take advantages of both waveguide and microstrip structures, such as low loss, high power capacity, low cost and easy to integrate in the planar circuit [6-8]. At high operating frequency as Ku-band, the use of SIW is a better choice to design a six-port structure compared to the microstrip technique because the loss contributed by the conductor is low in SIW since the signal is travelling inside the substrate [9]. Unlike in microstrip structure, some of the electric fields is propagating in the air; increasing the losses as the frequency increasing.

There are some six-port SIW works that are available in the open literature. For instance, the SIW six-port work was successfully demonstrated in [10], employing a dual-layered technique to achieve a compact dimension. Despite its excellent performance, the fabrication of the multi-layer SIW technology is somewhat sensitive, the presence of air-gaps between the layers and the misalignment of the different layers that could cause a degradation in the measured performance of the fabricated device.

Next, a single layer SIW six-port device was presented in [11] but the demonstration is limited to the simulation. In [12-13], the proposed single layer SIW six-port structures were verified experimentally, however, the configuration of the SIW six-port device has more than six ports; seven- or eight ports, in which the unused ports should be terminated by appropriate loads.

Therefore, a single layer SIW six-port junction working in Ku-band is presented in this paper. This work is motivated by the presented single layer SIW six-port device operating at K-Band in [14] that proposes six-port topology with no excessive port. In this paper, different configuration of coupler is applied in the six-port design to obtain a flat response of the transmission coefficient and the phase difference of the output ports across the Ku-band frequency range. As the key components of the six-port device are the power dividers and couplers, the design of each component is presented in detail in the following sub-section. All the components including the final six-port junction are constructed on the RO4003C substrate, having the dielectric constant, ϵ_r of 3.38 and the thickness, h of 0.508 mm.

2. RESEARCH METHOD

The chosen schematic topology of the proposed SIW six-port is shown in Figure 1. The six-port junction presented in this paper is constructed by two power dividers, two hybrid couplers and $\pm 45^\circ$ phase shifters. As demonstrated in [14], this topology is compact in size and does not require any external connecting terminals like the traditional six-ports presented in [12-13].

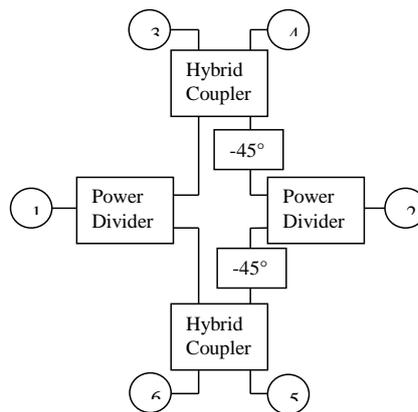


Figure 1. Topology of the six-port

As per the design modelling of SIW given in [15], the corresponding resonant frequency, $f_{c(TE_{10})}$ for SIW is used to determine the width of SIW, W_{eff} . The width of SIW power divider and SIW coupler, W_{eff} is determined by the mathematical expression (1) and (2):

$$f_{c(TE_{10})} = \frac{c}{2\sqrt{\epsilon_r}} \cdot \left(W - \frac{d^2}{0.95 \cdot p} \right)^{-1} \quad (1)$$

$$W_{eff} = W - \frac{d^2}{0.95 \cdot p} \quad (2)$$

where c is the speed of light, ϵ_r is the dielectric constant, W is the width of waveguide port, d is the via holes diameter and p is the distance between via holes (centre to centre). In order to achieve an excellent performance of the proposed SIW, a few design rules regarding the via holes, as written in expression (3) to (5) need to be followed [16-17].

$$\frac{p}{\lambda_c} < 0.25 \tag{3}$$

$$d < \frac{\lambda_g}{5} \tag{4}$$

$$d < p < 2d \tag{5}$$

where λ_c is the wavelength of the cutoff frequency, $f_{c(TE10)}$ and λ_g guided wavelength of the standard operating frequency.

The SIW power divider is designed based on Y-junction topology[18], where the details design guidelines shown in [19]. The length of l_1 and l_3 is set to be enough to perform as the transmission line in SIW mode. The length of l_2 is optimized to obtain low reflection coefficient S_{11} and transmission coefficients S_{21} and S_{31} close to -3 dB.

For SIW coupler, the electrical coupling strength is achieved by coupling two SIW lines with similar dimensions via a suitable aperture. Compared to the traditional SIW couplers [20-24], the presented coupler configuration in this paper is modified where the position of a row of several vias at the centre with a length, l_p is shifted by the parameter c_a , closer to the side walls. This will gives a wider width at the centre of coupler structure between two rows of the parallel vias. As a result, the amplitude imbalance is reduced, giving a more flat response of the coupling coefficient. The length of l_1 and l_3 is set to be enough to perform as the transmission line in SIW mode. The length of l_2 is optimized to obtain low reflection coefficient S_{11} , low isolation coefficient S_{41} and transmission coefficients S_{21} and S_{31} close to -3 dB. The length of l_2 managed to obtain the required performance of S_{11} and S_{41} but the S_{31} is larger than S_{21} . The l_p and c_a is optimized to adjust the power division between S_{21} and S_{31} to be possibly equal. Both increase of l_p and c_a has increased the S_{21} but decrease the S_{31} performance. As a result, the S_{21} and S_{31} have almost equal power division. Optimization has been done for both SIW power divider and SIW coupler using the electromagnetic simulation tool and the parameters values are shown in Figure 2.

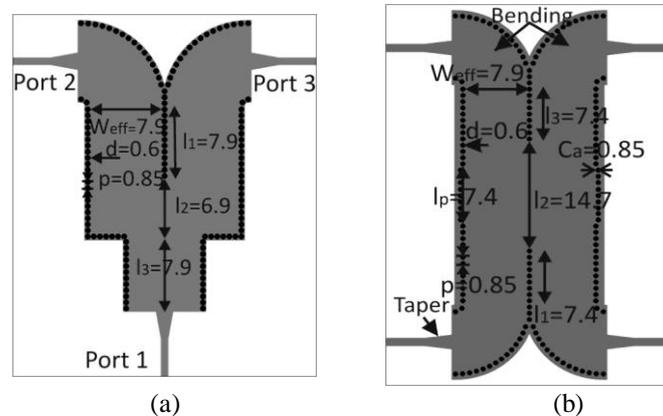


Figure 2. Geometric configuration and the parameters of (a) SIW power divider and (b) SIW coupler in mm

The SIW six-port layout is shown in Figure 3. As shown in Figure 3, each bend is designed to connect SIW power divider and SIW coupler. The bending line width is set to be similar to the W_{eff} . The bending has cause some shifting in the operating frequency and introduces little insertion loss. The bending is first designed on SIW power divider and SIW coupler before combined to form SIW six-port. The designed six-port should obtain low reflection coefficient S_{11} and S_{22} , and also good isolation S_{21} . The transmission S_{31} to S_{61} and S_{32} to S_{62} should be close to -6 dB. Since the gaps between port 3 and port 4, and also port 5 and port 6 do not have wide gaps, the connection between the connectors during measurement might be a problem. Therefore, bends are designed for all the output ports to solve this potential problem occurs. The taper is added to improve the matching between the transition SIW to the microstrip line. The initial width is determined first based on [25] and the length of the taper is optimized using a electromagnetic simulation tool to obtain low reflection coefficient and minimize the insertion loss at each port. The extension of the microstrip line is done on port 3, port 4, port 5 and port 6 for easy board cutting

process since the PCB board cutting machine available can only perform the direct straight cut. The -45° and 45° phase different is performed by shifting the SIW power divider at port 2 towards the SIW coupler at the left hand side. This results in a reduction of SIW transmission line on one side (-45° phase shift) and addition of SIW transmission line on the other side (45° phase shift) of the SIW coupler to form the SIW six-port. The optimization is done by using the electromagnetic simulation tool to obtain the phase different between port 3 and port 4, and also port 5 and port 6 close to 90°

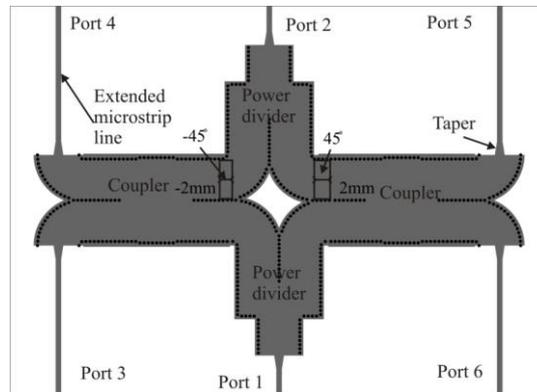


Figure 3. SIW six-port structure highlighting the phase shifts produced due to the addition of transmission lines

3. RESULTS AND ANALYSIS

This section provides the analysis of coupler performance in terms of S-parameters such as reflected coefficient, transmission coefficient and the phase differences between the output ports. Based on the optimized design parameters obtained in the previous sections, the structure was simulated and then fabricated to validate the proposed design, as shown in Figure 4. The fabricated prototype of SIW power divider, coupler and six-port are measured using Agilent vector network analyzer E8362B. The simulation and measurement results are discussed in the following sections.

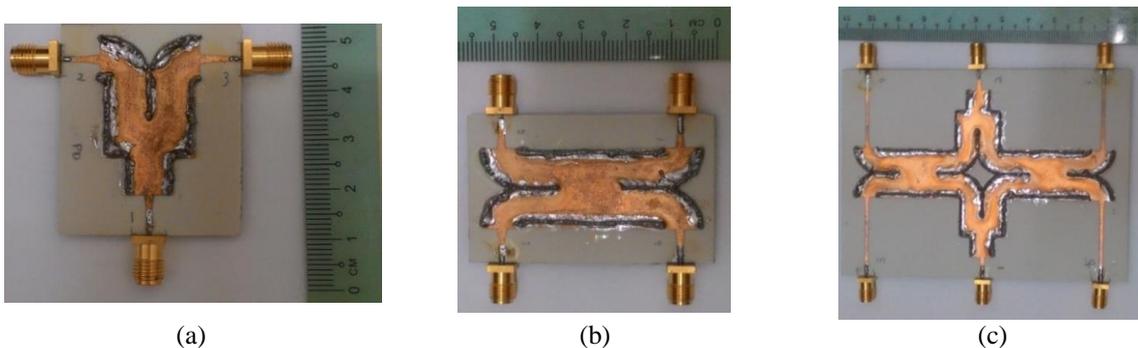


Figure 4. Photograph of the fabricated (a) SIW power divider, (b) SIW hybrid coupler, (c) SIW six-port

3.1. Simulation and Measurement Results of SIW Power Divider

The comparison between the simulation and measurement results of the SIW power divider is shown in Figure 5. As depicted in Figure 5(a), the simulated return loss is better than 15 dB over 13 to 17 GHz while the measured return loss is better than 9 dB within the same frequency range. The simulated S_{21} shown in Figure 5(b) demonstrate a flat response of the output power division with 3.5 ± 0.1 dB can be observed across the intended frequency range from 13 to 17 GHz. The measured result of S_{21} is 5 ± 1 dB across the same frequency range. The degradation of the fabricated prototypes performance might be contributed by the leakage of the propagating signal through the vias due to imperfect conduction of vias holes.

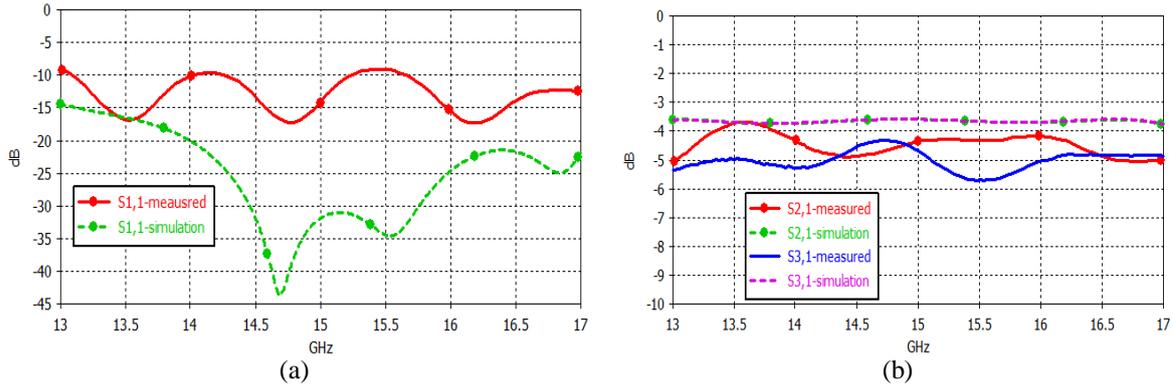


Figure 5. Comparison between simulation and measurement results of SIW power divider (a) S_{11} , (b) S_{21} , S_{31} .

3.2. Simulation and Measurement Results of SIW Hybrid Coupler

The comparison between the simulation and measurement results of designed SIW coupler is shown in Figure 6. The simulated and measured S_{11} and S_{41} is better than 15 dB across 13 to 16.8 GHz. The simulated S_{21} is approximately 3.8 ± 0.5 dB while the measured result is approximately 4.5 ± 0.5 dB within the operating frequency of 13 GHz to 16 GHz. There is a slight deviation in measured results as compared to the simulation which is mainly due to the SMA connector loss, measurement or fabrication errors. The measured results are in good agreement with the simulated results, except that there is slight frequency shift of approximately 1%.

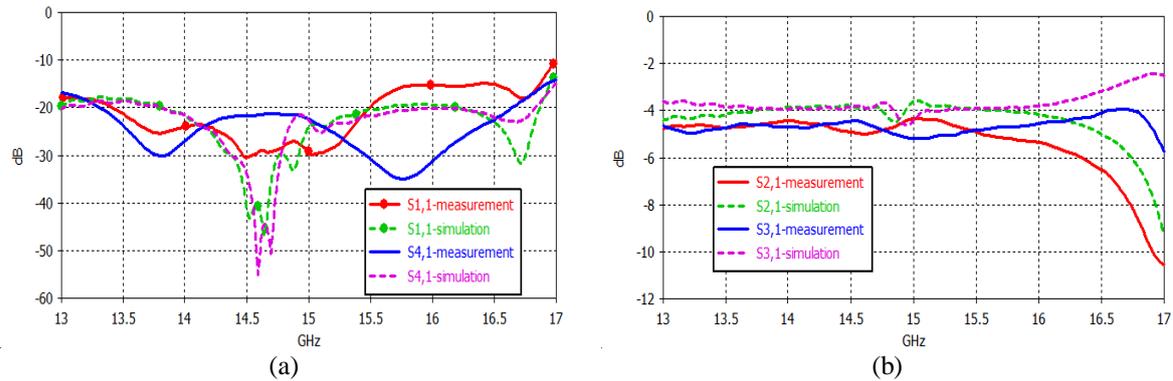


Figure 6. Comparison between simulation and measurement results of SIW hybrid coupler (a) S_{11}, S_{41} (b) S_{21}, S_{31} .

3.3. Simulation and Measurement Results of SIW Six-port

The simulation and measurement results are shown in Figure 7. The simulated and measured reflection coefficient, S_{11} and isolation, S_{21} is lower than -10 dB across 13.5 to 17 GHz as seen in Figure 7(a), respectively. The simulated results of transmission coefficient, S_{31} , S_{41} , S_{51} , and S_{61} are about -7 ± 1.5 dB across the operating frequency range of 13 GHz to 16.5 GHz. The measured results of S_{31} is -10 ± 2 dB over 13 GHz to 16.5 GHz while for S_{41} , S_{51} , and S_{61} are -9 ± 1 dB across the same frequency range as shown in Figure 7(b).

Figure 8 shows the phase difference between the different ports of the SIW six-port device within the frequency range of 13 - 16.5 GHz. The SIW six-port accomplished to achieve simulated phase difference between port 5 and port 6 of $90^\circ \pm 5^\circ$.

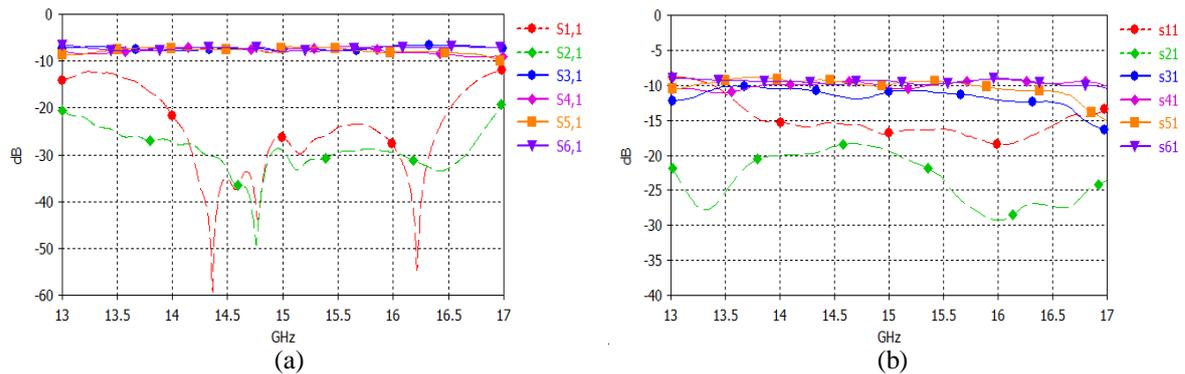


Figure 7. (a) Simulation and (b) Measurement results of SIW Six-port

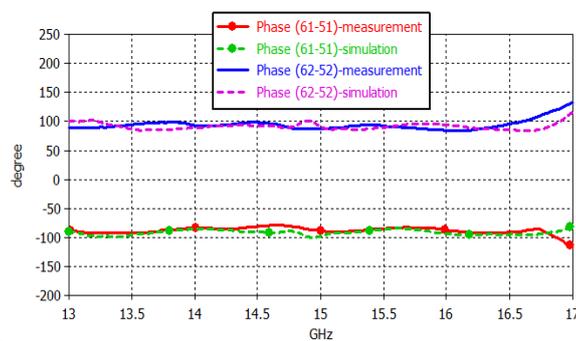


Figure 8. Comparison of simulation and measurement phase differences of SIW six-port

4. CONCLUSION

In this paper, a single layer Ku-band power divider, hybrid coupler, and six-port using SIW technology have been designed and fabricated. The chosen topology of the SIW six-port has no excessive ports. The simulated and measured results of the modified SIW hybrid coupler show that it has advantage of flat response of the coupling coefficient contributed by the modification of the position of a row of several vias at the centre of the side walls. The measurement results demonstrate that the combination of the Y-junction SIW power divider and the proposed SIW hybrid coupler can lead to design of SIW six-port operating in Ku-band. Good agreement between the measurements and simulations is obtained.

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