

Low voltage CMOS power amplifier with integrated analog Pre-Distorter for BLE 4.0 application

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ABSTRACT

In this paper, a low power consumption linear power amplifier (PA) for Bluetooth Low Energy (BLE) application is presented. An analogue pre-distorter (APD) is integrated to the PA. The APD consist of an active inductor, driver amplifier, and a RC phase linearizer. The PA delivers more than 12dB power gain from 2.4GHz to 2.5GHz. At the center frequency of 2.45GHz, the gain of the PA is 13dB with PAE of 26.7% and maximum output power of 14dBm. The corresponding OIP3 is 27.6dBm. The supply voltage headroom of this PA is 1.8V. The propose APD serves to be a solution to improve the linearity of the PA with minimum trade-off to the power consumption.

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1. INTRODUCTION

In recent years, wireless communication system has evolved rapidly to accomplish higher data rate transmission scheme. Wireless communication is aiding in the development of Internet of Things (IoT) which includes communication devices such as Wi-Fi, Zigbee, and Bluetooth.

Bluetooth devices work in the Industrial, Scientific, and Medical (ISM) band which is located at 2.4 – 2.483 GHz. Bluetooth devices is classified into 3 classes based on their data transmission distance. Higher transmission distance requires higher output power from the transmitter. The classes are Class 1, Class2, and Class 3 with maximum output power of 20dBm, 4dBm, and 0dBm respectively [1]. Bluetooth power amplifier usually works in low power mode, which requires the Class 1 power amplifier to be controlled down to 4dBm or less in a monotonic sequence in order to save the power [2]. Figure 1 depicts the location of the PA in the block diagram of BLE transmitter.

CMOS power amplifier have been broadly examined to satisfy the demand of low cost and minimal size transceivers. Due to the high tradeoff between linearity and efficiency in CMOS PAs as compared to GaAs PAs, arduous challenges have been faced in order to achieve stringent linearity requirements for modern wireless communication system [3-6]. Various intrinsic drawbacks in CMOS PA such as low quality factor, lossy substrate of passive structures, low breakdown voltage, and low trans-conductance of active devices contributes to the difficulty of CMOS PA commercialization. Therefore, numerous exertions

in terms of linearity enhancement techniques and efficiency enhancement techniques have been implemented on overcoming the drawbacks of CMOS technology for PA designs [7-9].

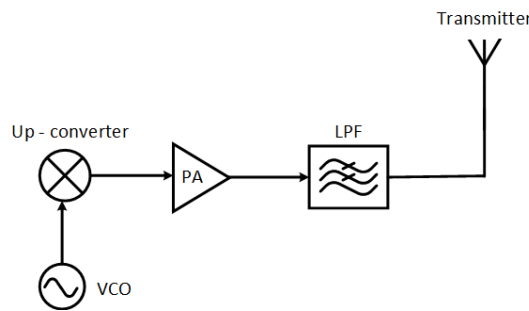


Figure 1. The block diagram of BLE transmitter

A simple linearization technique using passive components have been proposed by P. Gunasegaran et al (2017) for BLE application [10]. A simple RC network is connected at the gate of the transistors which reduces C_{gs} effect and thus improves linearity. Moreover, linearization using a simple body network have been proposed by G. Jeong et al (2016) for WLAN application [11]. A linearizing body network is implemented by utilizing a resistor that connect the body and drain node of a power transistor. Also, a common-gate combining PA with load impedance adaptor have been proposed by Y. Jin et al (2017) [12]. The PA is utilized for WLAN application in which the main amplifiers are biased differently to apply the adaptive power cell technique which enhances linearity.

The purpose of this work is to design a linear low power CMOS PA for BLE application. High linearity is targeted to enhance the communication distance while preserving the quality of the data transmitted. An analogue pre-distorter is implemented in the CMOS PA to achieve this target. The outline of this work is arranged as follows. In Section 2, the design methodology of the CMOS PA is described. Section 3 represents the post layout results obtained for the designed CMOS PA. Finally, the conclusion is presented in Section 4.

2. DESIGN METHODOLOGY

The schematic diagram of the proposed CMOS power amplifier (PA) with APD is illustrated in Figure 2. Z_{out} APD denotes the output impedance of the APD while Z_{out} Main denotes the output impedance of the main amplifier. The main amplifier is biased at Class AB with quiescent current of 17 mA. The input matching network is represented by C1, C2, C3, and L1. On the other hand, the output matching network is represented by C11, C12, C13, and L3. Capacitor C10 functions as a decoupling capacitor to shunt the third order non-linear component produced from the drain supply to ground. Inductor L2 and capacitor C9 nullifies the effect of parasitic drain-source capacitance, C_{ds} , thus improving the PAE of the PA.

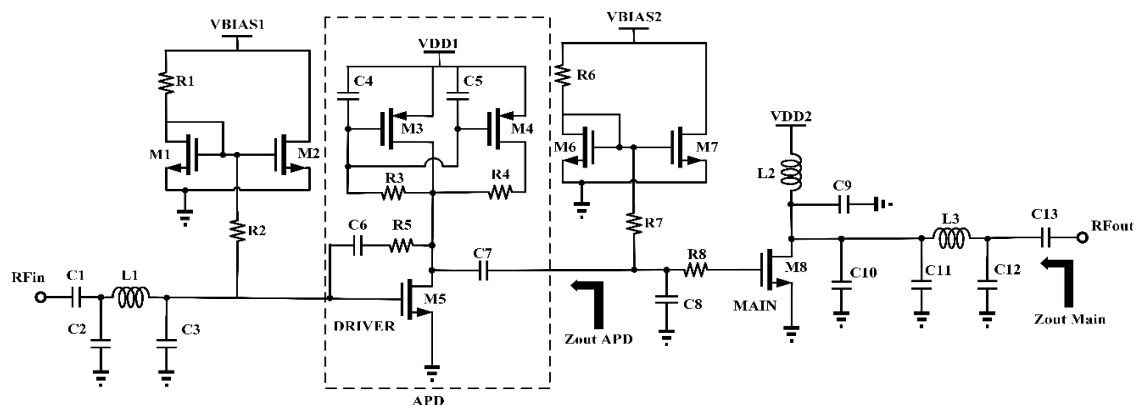


Figure 2. The schematic of the PA with APD

Figure 3 depicts the AM – PM responses of the APD and main amplifier. The phase response between the APD and main amplifier are opposite to each other and is represented in 1 and 2 respectively.

$$\begin{aligned}
 & [(R_5R_3R_{o1}R_{o2}R_{o3}R_8 + R_5R_3R_4R_{o1}R_{o3}R_8) - j\omega(C_8R_5R_3R_{o1}R_{o2}R_{o3} + C_8R_5R_3R_4R_{o1}R_{o3} \\
 & + C_8R_3R_8R_{o1}R_{o2} + C_7R_3R_8R_{o1}R_{o2} + C_7R_3R_4R_8R_{o1} + C_7R_5R_8R_{o1}R_{o2} + C_7R_5R_8R_4R_{o1} \\
 & + C_7R_3R_5R_8R_{o2} + C_7R_3R_4R_5R_8 + C_7R_3R_5R_8R_{o1} + C_7R_8R_{o3} + C_6R_3R_8R_{o1}R_{o2}R_{o3} \\
 & + C_6R_3R_4R_8R_{o1}R_{o3})]
 \end{aligned} \tag{1}$$

$$\begin{aligned}
 Z_{out_APD} = & \frac{[(R_5R_3R_{o1}R_{o2}R_{o3} + R_5R_3R_4R_{o1}R_{o3}) - j\omega(C_6R_{o1}R_{o2}R_{o3}R_3 + C_6R_3R_4R_{o1}R_{o3} + C_7R_{o1}R_{o2}R_3 \\
 & + C_7R_{o1}R_4R_3 + C_7C_3R_5R_{o1}R_{o2} + C_7C_3R_{o3}R_4 + C_7R_5R_3R_{o2} + C_7R_3R_4R_5 + C_7R_3R_5R_{o1} \\
 & + C_7R_{o3} + C_8R_{o1}R_{o2}R_3 + C_8R_{o1}R_4R_3 + C_8R_{o1}R_{o2}R_5 + C_8R_{o1}R_4R_5 + C_8R_{o2}R_3R_5 \\
 & + C_8R_3R_4R_5 + C_8R_3R_5R_{o1} + C_8R_{o3})]}{
 \end{aligned}$$

where R_{o1} , R_{o2} , and R_{o3} are the resistor representation of the channel length modulation of transistors M3, M4, and M5 respectively.

$$\begin{aligned}
 & j\omega(C_{10}C_{11}C_{12}R_{o4} + C_{10}C_{11}C_{13}R_{o4} + C_{10}C_{12}C_{13}R_{o4} - C_{10}C_{12}L_3R_{o4} \\
 & - C_{10}C_{13}L_3R_{o4} + C_{11}C_{12}C_{13}R_{o4} - C_{11}C_{12}L_3R_{o4} - C_{11}C_{13}L_3R_{o4})
 \end{aligned} \tag{2}$$

$$\begin{aligned}
 Z_{out_MAIN} = & \frac{[(C_{11}L_3R_{o4} - C_{11}C_{12}R_{o4} + C_{10}L_3R_{o4} - C_{10}C_{12}R_{o4} \\
 & - C_{11}C_{13}R_{o4}) + j\omega(C_{10}C_{11}C_{12} - C_{10}C_{11}L_3)]{
 \end{aligned}$$

where R_{o4} is the resistor representation of channel length modulation of transistor M8.

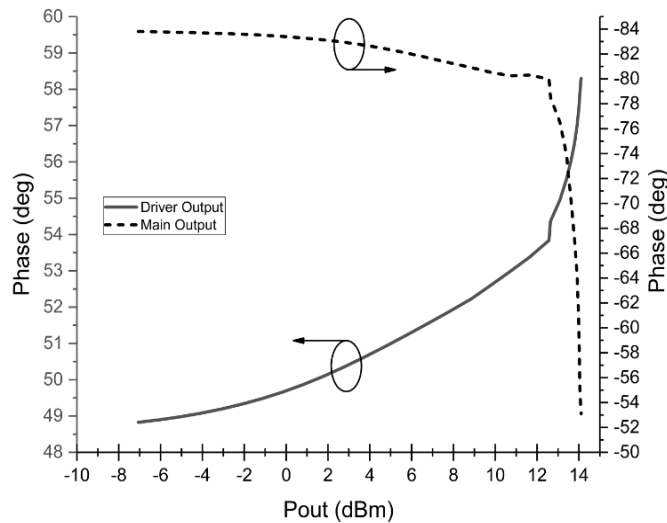


Figure 3. The AM-PM responses of the APD and main amplifier

3. VALIDATION RESULTS

The small signal parameters of the PA is as shown in Figure 4. At the center frequency of 2.45GHz, the PA produces a gain of 13dB. The S11 and S22 value of the PA are -19.5dB and -19.7dB respectively which provides a good reverse isolation of both input and output.

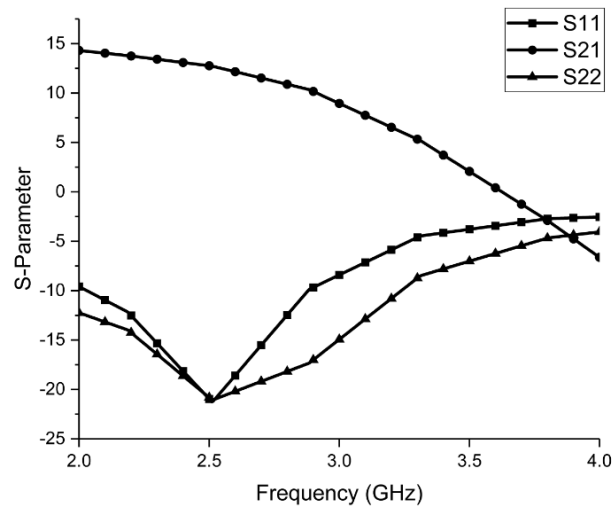


Figure 4. Small signal parameters of the designed PA

The stability factor of the PA is depicted in Figure 5. It can be observed from the figure that the PA is unconditionally stable across the frequency of 1GHz to 5GHz.

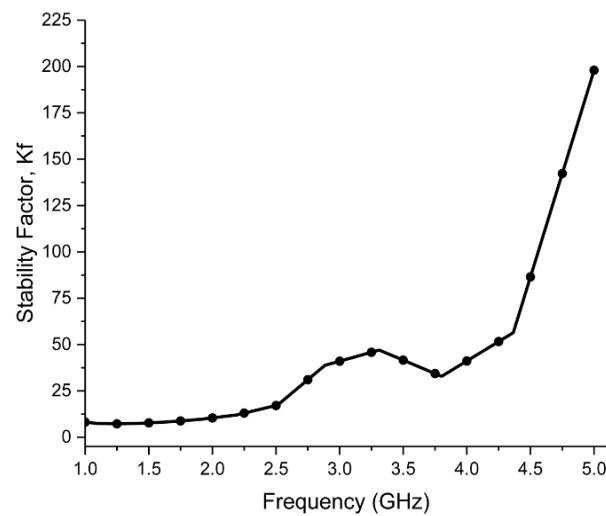


Figure 5. The stability factor of the PA is unconditionally stable

Figure 6 shows power gain, PAE, and OIP3 of the PA. The power gain of the PA across output power shows a flat gain is achieved up to 1dB compression point. The maximum delivered output power is 14.1dBm while the 1dB compressed output power (P_{1dB}) is 12.6dBm. The PA achieves a peak power added efficiency (PAE) of 26.7% at the center frequency of 2.45GHz. In addition, the linearity of the PA is presented in terms of output third order intermodulation product (OIP3). The PA produces maximum OIP3 of 27.6dBm when a dual tone signal with 1MHz spacing is injected to the input of the PA. At this point, the phase cancellation is maximum.

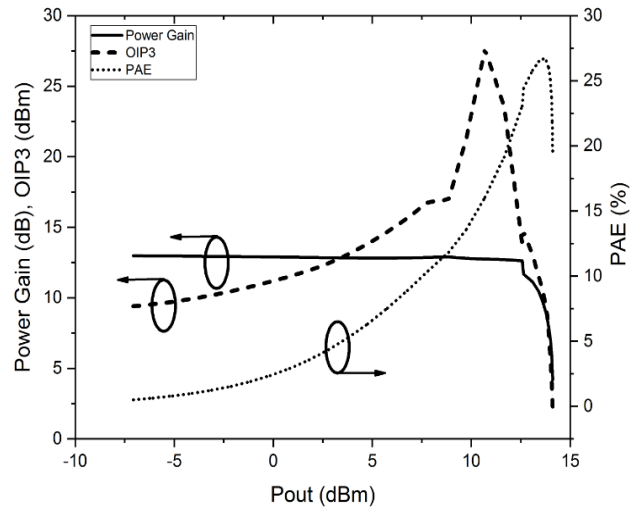


Figure 6. The power gain, PAE, and OIP3 achieved by the PA

The layout of the designed PA is depicted in Figure 7. The chip size of the PA is 1678um x 1748um including the pads for measurement. The post layout simulation performance of the PA is summarized in Table 1. On the other hand, the recent works on low power CMOS PA is summarized and compared in Table 2.

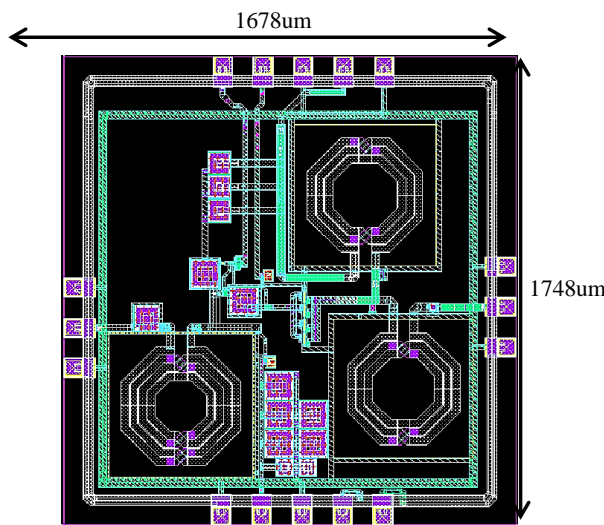


Figure 7. The layout of the designed PA

Table 1. Post Layout Simulation Performance of the PA

Operating Frequency	2.45GHz
Bandwidth	100MHz
Power Gain, S21	12.9dB
Input Return Loss, S11	-19.5dB
Output Return Loss, S22	-19.7dB
Peak PAE	26.7%
Max. Output Power	14.1dBm
OIP3	27.6dBm
Power Supply Voltage	1.8V
Technology	180nm CMOS

Table 2. Work Comparison with Published Power Amplifiers

Ref	PA Tech.	Supply (V)	Max Linear Pout (dBm)	Peak PAE (%)	Gain (dB)	Freq. (GHz)	Linearity	Application
[10]	180nm	1.8	13	38.4	10	2.45	20.6dBm (OIP3)	BLE
[11]	55nm	3.3	16	16	30	2.45	-34dBc (IMD3)	WLAN
[12]	180nm	3.3	22.08	31.97	30.7	2.4	-	WLAN
[13]	130nm	2.0	19	32	31	2.5	-	-
[14]	180nm	3.3	16.5	36.6	22	0.6	-	IoT
This work	180nm	1.8	12.6	27.6	13	2.45	27.6dBm	BLE

4. CONCLUSION

In this paper, an 180nm CMOS PA was designed with an integrated analogue pre-distorter (APD) in which an active inductor is a part of it. The APD improves the linear output power of the PA for low power BLE power amplifier. The PA achieved an OIP3 of 27.6dBm with maximum PAE of 26.7%, as well as maximum output power of 14.1dBm. Hence, the proposed PA design serves as a good solution to be integrated with a low power BLE transceiver.


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